



Calhoun: The NPS Institutional Archive

Theses and Dissertations

Thesis Collection

1949

Gain margin, phase margin and transient response
of some simple servomechanisms.

Hunnicut, William R.

Cornell University

<http://hdl.handle.net/10945/6418>



Calhoun is a project of the Dudley Knox Library at NPS, furthering the precepts and goals of open government and government transparency. All information contained herein has been approved for release by the NPS Public Affairs Officer.

Dudley Knox Library / Naval Postgraduate School
411 Dyer Road / 1 University Circle
Monterey, California USA 93943

<http://www.nps.edu/library>

NPS ARCHIVE
1949
HUNNICUTT, W.



Thesis
H93

GAUSS, ELLIPTIC, and TRANSIENT RESPONSE
OF SOME SIMPLE CIRCuits

by

William R. Hannicutt, Jr.

B.S. in Electrical Engineering

U.S. Naval Academy 1932

Presented to the Moore School of Electrical
Engineering of the University of Pennsylvania
as partial fulfillment of the requirements for
the Degree of Master of Science in Electrical
Engineering. May 1949

DUDLEY KNOX LIBRARY
NAVAL POSTGRADUATE SCHOOL
MONTEREY, CA 93943-5101

Library
U. S. Naval Postgraduate School
Monterey, Md.

TABLE OF CONTENTS

SUBJECT	PAGE
Introduction	2
Theory and Derivations	2
Calculation of Phase and Gain Margins	4
Transient Response	8
Discussion	12
Appendix (1) Nomenclature	14
Appendix (2) Bibliography	15
Appendix (3) Data Sheets	16

	Curve
Effect of variation of input under saturated conditions	A-1
Phase and Gain Margins, transfer function (F)	B-1
Maximum overshoot d. transfer function (B)	B-2
Time τ as a function of α , transfer function (B)	B-3
Maximum overshoot d vs α , transfer function (B)	B-4
Phase and Gain Margins, transfer function (C)	C-1 through C-4
Maximum overshoot d, transfer function (C)	C-5
Time τ as a function of α and β	C-6 through C-9
Transient response, transfer functions (B) and (C)	D-1
Transient response, transfer functions (A), (B), (C).	D-2

Gain Margin and Phase Margin are frequently used as design criteria in servomechanism design inasmuch as they bound the transfer function of the system in the region of principal resonance of the overall function. (Ref. 2, Ch. 6-12)

This paper will consider some simple servomechanism transfer functions and show relations between Gain and Phase margins for systems using these transfer functions. Transient response to a step input will be considered as a function of phase margin.

Transient response was determined by means of the Moore-School Differential Analyzer. Due to availability of the differential analyzer this analysis is concerned with a non-linear servomechanism system in that the effective error signal cannot exceed one in value. The applied error signal \mathcal{E}_c will be 5, the saturated value of the error signal \mathcal{E}_c will equal one. This case is analogous to that in which the servo amplifier saturates at $\mathcal{E}_c = 1$ while $\theta_1 - \theta_0 = 5$.

TABLE OF CONTENTS

SUBJECT	PAGE
Introduction	2
Theory and Derivations	2
Calculation of Phase and Gain Margins	4
Transient Response	8
Discussion	12
Appendix (1) Nomenclature	14
Appendix (2) Bibliography	15
Appendix (3) Data Sheets	16

	Curve
Effect of variation of input under saturated conditions	A-1
Phase and Gain Margins, transfer function (B)	B-1
Maximum overshoot d , transfer function (B)	B-2
Time T as a function of α , transfer function (B)	B-3
Maximum overshoot d vs K , transfer function (B)	B-4
Phase and Gain Margins, transfer function (C)	C-1 through C-4
Maximum overshoot d , transfer function (C)	C-5
Time T as a function of α and β	C-6 through C-9
Transient response, transfer functions (F) and (G)	D-1
Transient response, transfer functions (I), (E), (C).	D-2

Gain Margin and Phase Margin are frequently used as design criteria in servomechanism design inasmuch as they bound the transfer function of the system in the region of principal resonance of the overall function. (Ref. 2, Ch. 6-12)

This paper will consider some simple servomechanism transfer functions and show relations between Gain and Phase margins for systems using these transfer functions. Transient response to a step input will be considered as a function of phase margin.

Transient response was determined by means of the Moore School Differential Analyzer. Due to availability of the differential analyzer this analysis is concerned with a non-linear servomechanism system in that the effective error signal cannot exceed one in value. The applied error signal ξ_c will be 5, the saturated value of the error signal ξ_c' will equal one. This case is analogous to that in which the servo amplifier saturates at $\xi_c = 1$ while $\theta_1 - \theta_0 = 5$.

THEORY AND DERIVATIONS

A simple feedback system of the form shown may be considered to consist of an input θ_1 , an error measuring device A, a transfer function $KY(p)$ where $p = ju$, an output θ_0 and a feedback line.

Let $\theta_1 - \theta_0 = \varepsilon$. Then $\theta_0 = \varepsilon (KY(p)) = [KY(p)] [\theta_1 - \theta_0]$ or

$\theta_0 / \theta_1 = \frac{KY(p)}{1 + KY(p)}$. It has been shown (ref. c) that a transfer

function may be reduced to the form
$$\frac{A_0 + A_1 p + A_2 p^2 + \dots + A_m p^m}{B_0 + B_1 p + B_2 p^2 + \dots + B_n p^n}$$

The transfer functions considered herein will be of the form:

$$(A) \quad KY(p) = \frac{K}{p(p+1)}$$

$$(B) \quad KY(p) = \frac{K}{p(p+1)(\alpha p+1)}$$

$$(C) \quad KY(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$

These transfer functions might arise as follows:

(A) Components (a) synchro transformer $E(j\omega) / \varepsilon(j\omega) = K_1$

(b) D.C. motor with shunt field control

$$\theta_0 / I_f = \frac{K_2}{(j\omega)(j\omega\tau+1)}$$

(c) electronic amplifier

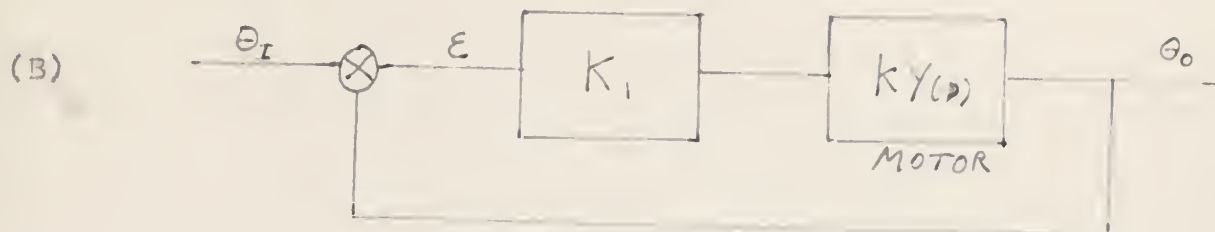
$$\text{Here } \theta_0 / \varepsilon = \frac{K_1 K_2}{j\omega(j\omega\tau+1)}$$

Substituting the Laplace transform form of eq. (b), let $\omega\tau = p$, then

$$\theta_0 / \varepsilon = \frac{K_1 K_2 \tau}{p(p+1)} = \frac{K}{p(p+1)} = KY(p) \quad p = ju$$

For (c) the amplifier the value of the factor $K_1 K_2 \tau$ is unity. Hence, the transfer function is as given above.

Transfer functions (B) and (C) may be similarly derived, for example



$$KY(j\omega) = \frac{K_1 K_2 K_f / R_f f}{j\omega(\tau_f j\omega + 1)(\tau_m j\omega + 1)} = \frac{K_1 K_2 K_f / R_f f}{j\omega(j\omega\tau_f + 1)(j\omega\tau_m + 1)}$$

arranging τ 's in order of size largest τ being τ_1 .

Let $\omega\tau_1 = u$, then $KY(ju) = \frac{K}{ju(ju+1)(ju\alpha+1)}$

where $\alpha = \frac{\tau_m}{\tau_f}$. Note that $\alpha \leq 1$.

Expression (C) may be similarly obtained. Thus, in the following discussion α and β will have values $0 \leq \alpha \leq 1$; $0 \leq \beta \leq 1$.

The transient response of systems having transfer functions of these forms may be obtained by means of the Laplace transform. Thus for expression (A):

$$\theta_o/\theta_i = \frac{KY(p)}{1+KY(p)} = \frac{K}{p(p+1) + K}$$

For θ_i a step function and $K = 1$,

$$\theta_o(p) = \frac{1}{p(p^2+p+1)} = \frac{1}{p[(p+\frac{1}{2})^2 + \frac{3}{4}]}$$

whence (form 1.304), ref(d).

$$\theta_o(t) = 1 + \frac{2}{\sqrt{3}} e^{-\frac{1}{2}t} \sin(\sqrt{3}/2 t - \psi) \text{ where } \psi = \tan^{-1} \sqrt{3}.$$

Where a large number of transient responses are required it is convenient to use the differential analyzer. This problem may be set up using the operator $p = d\theta/dt$. For the transfer function

(A) $KY(p) = \frac{K}{p(p+1)} = \theta_o/\epsilon$.

$$p(p+1)\theta_o = K\epsilon \quad (d^2\theta_o/dt^2 + d\theta_o/dt) = K\epsilon$$

$$\epsilon = \theta_i - \theta_o \quad \text{For } \theta_i \text{ a constant } (d^2\theta_o/dt^2 + d\theta_o/dt) = -(\frac{d^2}{dt^2} + \frac{d}{dt})\theta_o = -(\frac{d^2}{dt^2} + \frac{d}{dt})\theta_o$$

then $-\left(\frac{d^2}{dt^2} + \frac{d}{dt}\right) \varepsilon(t) = K \varepsilon(t)$ The solution to this equation gives $\varepsilon(t)$ whence $\theta_0(t) = 1 - \varepsilon(t)$

For expression (B) $KY(p) = \frac{K}{p(p+1)(\alpha p+1)} = \theta_0/\varepsilon$

$$[\alpha p^3 + (1+\alpha)p^2 + p] \theta_0(t) = K \varepsilon(t)$$

$$-[\alpha p^3 + (1+\alpha)p^2 + p] \varepsilon(t) = K \varepsilon(t)$$

the solution of which gives

$$\varepsilon(t), \text{ whence } \theta_0(t) = 1 - \varepsilon(t)$$

For expression (C) $KY(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$

$$\theta_0/\varepsilon = \frac{K}{\alpha \beta p^4 + (\alpha \beta + \alpha + \beta)p^3 + (\alpha + \beta + 1)p^2 + p}$$

$$-[\alpha \beta p^4 + (\alpha \beta + \alpha + \beta)p^3 + (\alpha + \beta + 1)p^2 + p] \varepsilon(t) = K \varepsilon(t)$$

$$\text{whence } \theta_0(t) = 1 - \varepsilon(t)$$

As transient response to a step input will be discussed in terms of gain margin and phase margin these will be defined as:

(a) Gain Margin: $1 - |KY(p)|$ at the point where the angle of $KY(p)$ equals 180° .

(b) Phase Margin: angle of $KY(p)$ diminished by 180° at the point where $|KY(p)| = 1$.

The servomechanisms considered will have the transfer functions:

$$(A) \quad KY(p) = \frac{K}{p(p+1)}$$

$$(B) \quad KY(p) = \frac{K}{p(p+1)(\alpha p+1)}$$

$$(C) \quad KY(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$

Their transient responses to a step input will be discussed as functions of phase margin and the relations between gain and phase margins for various values of α , β , and K will be shown. As previously stated, these servomechanisms will be considered to be non-linear in that the effective error signal cannot exceed one. The applied error signal \mathcal{E}_0 will be 5, the saturated value of the error signal \mathcal{E}_c will equal one. The effects of saturation on transient response are shown in Curve A-1.

To show the relations between gain and phase margins and the transient response to a step input it is necessary to determine the K required for each value of gain and phase margin considered. This is done by solving for the frequency u required to obtain the proper angle of $KY(p)$, then substituting this value in $KY(p)$ to determine K .

For expression (A) it is seen that gain margin does not exist since the locus of $KY(p)$ does not cross the 180° axis. At the point at which phase margin is measured,

$$|KY(p)| = \left| \frac{K}{p(p+1)} \right| = \left| \frac{K}{ju(ju+1)} \right| = 1$$

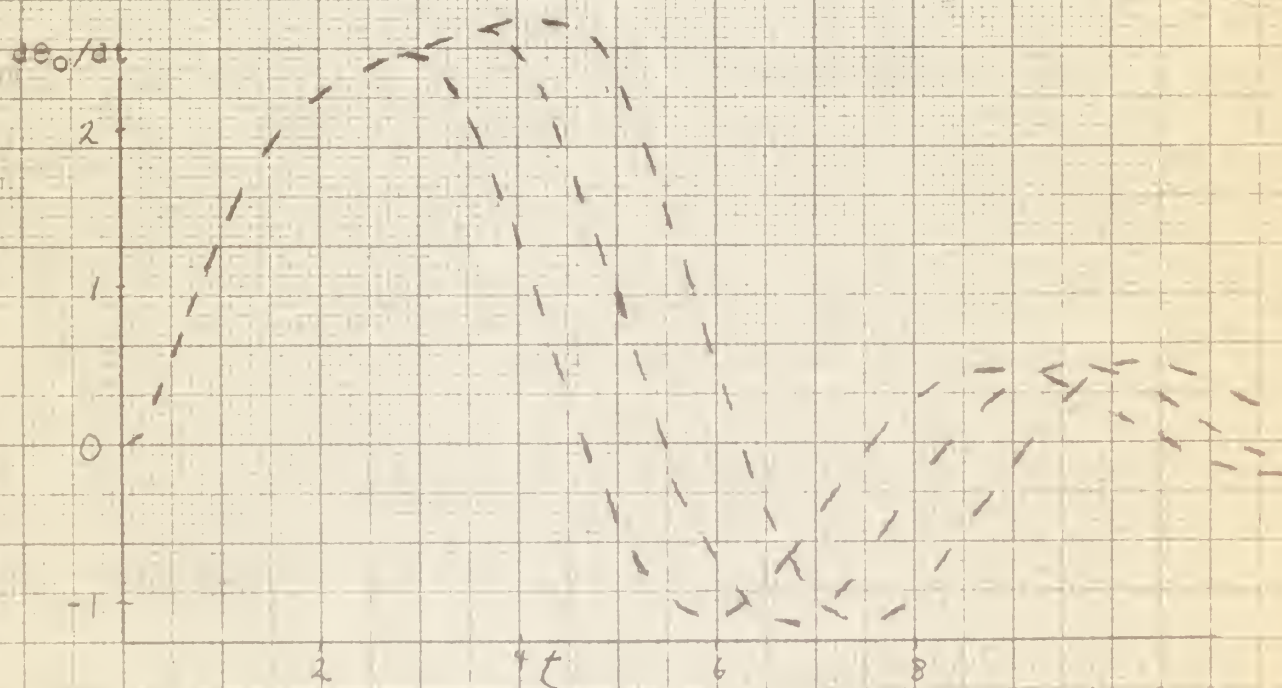
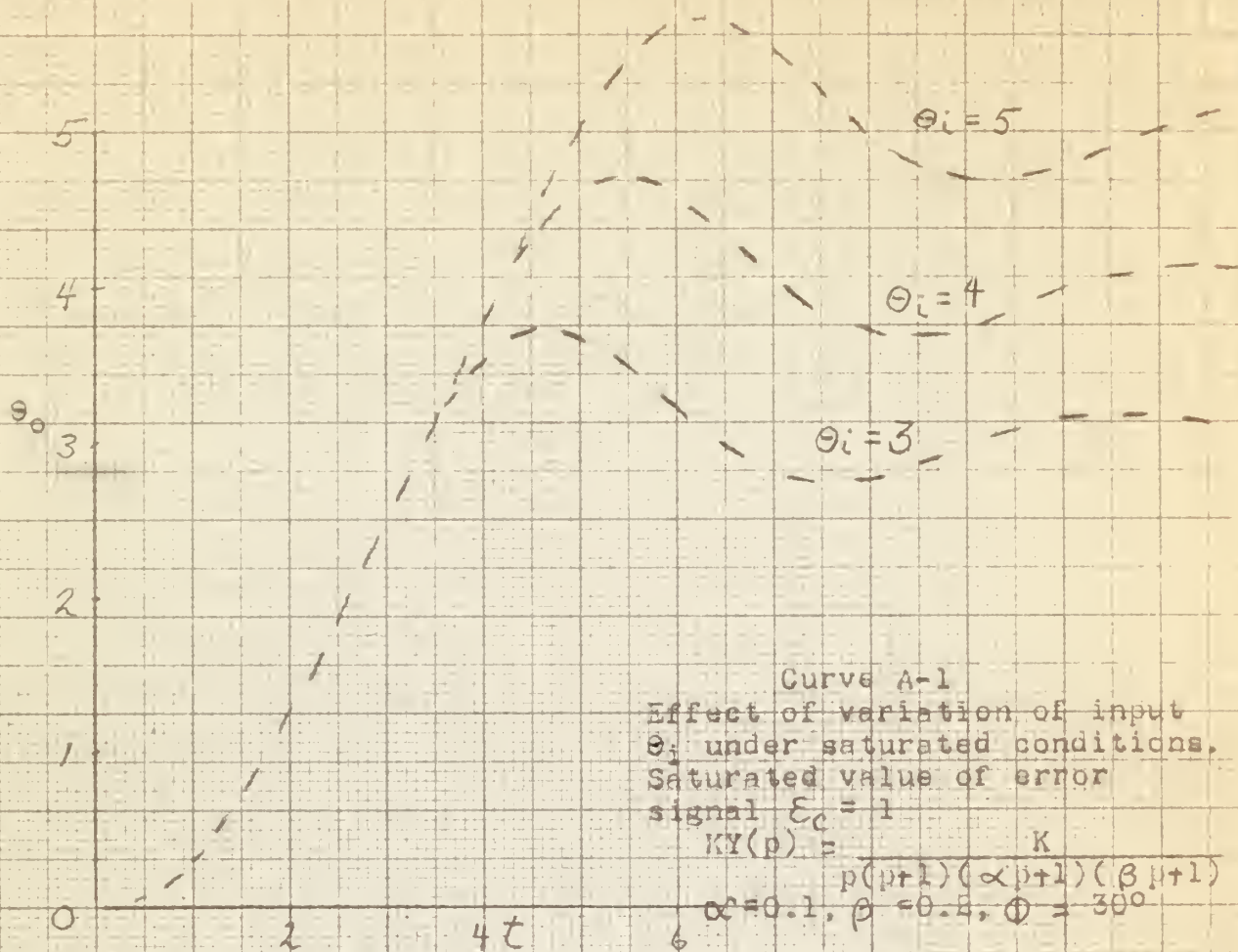
$$K = |u\sqrt{u^2+1}| \quad \text{angle } KY(p) = -90 - \tan^{-1}u$$

$$\text{phase margin } \phi = \angle KY(p) - 180$$

$$= -90 - \tan^{-1}u - 180$$

$$= -270 - \tan^{-1}u \text{ or } \tan(\phi + 270) = -u_0$$

$$\cot \phi = u_0 \quad \text{then } K = u_0 \sqrt{u_0^2 + 1}$$



Expression (B)

$$\text{Phase Margin: } KY(p) = \frac{K}{p(p+1)(\alpha p+1)} = \frac{K}{ju(ju+1)(j\alpha u+1)}$$

$$\angle KY(p) = \theta = -90 - \tan^{-1}u - \tan^{-1}\alpha u$$

$$\text{phase margin } \Phi = -90 - \tan^{-1} \frac{u(1+\alpha)}{1-\alpha u^2} - 180$$

$$\tan(\Phi + 270) = -\cot \Phi = \frac{-u(1+\alpha)}{1-\alpha u^2}$$

$$\cot \Phi - \alpha u^2 \cot \Phi - u(1+\alpha) = 0$$

$$u^2 + u \frac{(1+\alpha)}{\alpha} \tan \Phi - 1/\alpha = 0$$

Substitution of the various phase margins Φ and α 's

considered and solution for u gives u_0 for the desired

$$\begin{aligned} \text{phase margin. Then: } |KY(ju_0)| &= 1 = \frac{K}{u_0(u_0^2+1)^{1/2}(\alpha^2 u_0^2+1)^{1/2}} \\ &= \frac{K \cos \theta_1 \cos \theta_2}{u_0} \end{aligned}$$

$$\text{or } K = \frac{u_0}{\cos \theta_1 \cos \theta_2} \quad \text{where } \theta_1 = \tan^{-1} u_0, \theta_2 = \tan^{-1} \alpha u_0$$

gives the value of K for the desired phase margin Φ .

Gain Margin:

$$\text{gain margin} = 1 - |KY(p)| \quad \text{where } \angle KY(p) = 180^\circ$$

$$\angle KY(p) = -90 - \tan^{-1} u - \tan^{-1} \alpha u = 180$$

$$\tan^{-1} u + \tan^{-1} \alpha u = -270 \quad \tan \frac{u(1+\alpha)}{1-\alpha u^2} = -270$$

$$\frac{u(1+\alpha)}{1-\alpha u^2} = \tan(-270) = \tan 90 = \infty$$

$$\text{therefore } 1-\alpha u^2 = 0 \quad \text{or } \alpha u^2 = 1 \quad \text{whence } u_1 = \frac{1}{\sqrt{\alpha}}$$

$$\text{then } |KY(p)| = \frac{K}{u_1 \sqrt{u_1^2+1} \sqrt{\alpha^2 u_1^2+1}} = \frac{K \cos \theta_1 \cos \theta_2}{u_1}$$

$$\text{where } \theta_1 = \tan^{-1} u_1; \theta_2 = \tan^{-1} \alpha u_1$$

$$1 - |KY(ju_1)| = \text{gain margin}$$

Expression (C)

Phase Margin: $KY(ju) = \frac{K}{ju(ju+1)(j\alpha u+1)(j\beta u+1)}$

$$\angle KY(ju) = \theta = -90 - \tan^{-1}u - \tan^{-1}\alpha u - \tan^{-1}\beta u$$

$$\theta + 90 = -\tan^{-1}u - \tan^{-1} \frac{u(\alpha + \beta)}{1 - \alpha\beta u^2}$$

$$= -\tan^{-1} \frac{u + \frac{u(\alpha + \beta)}{1 - \alpha\beta u^2}}{1 - \frac{u^2(\alpha + \beta)}{1 - \alpha\beta u^2}}$$

$$\Phi = \theta - 180^\circ$$

$$\cot \Phi = \cot \theta = \frac{u(1 - \alpha\beta u^2) + u(\alpha + \beta)}{1 - \alpha\beta u^2 - u^2(\alpha + \beta)} \quad \text{which reduces to}$$

$$u^3 - \frac{u^2(\alpha\beta + \alpha + \beta)\cot\Phi}{\alpha\beta} - \frac{u(1 + \alpha + \beta)}{\alpha\beta} + \frac{\cot\Phi}{\alpha\beta} = 0$$

Solution for u for given values of Φ , α , and β gives u_0

Then, since $|KY(ju)| = 1$ at $u = u_0$

$$K = \frac{u_0}{\cos\theta_1 \cos\theta_2 \cos\theta_3}$$

$$\text{where } \theta_1 = \tan^{-1} u_0$$

$$\theta_2 = \tan^{-1} \alpha u_0$$

$$\theta_3 = \tan^{-1} \beta u_0$$

$$\begin{aligned} \text{Gain Margin:} \quad \text{Previously, } \cot \Phi &= \frac{u(1 - \alpha\beta u^2) + u(\alpha + \beta)}{1 - \alpha\beta u^2 - u^2(\alpha + \beta)} \\ &= \frac{u(1 - \alpha\beta u^2) + u(\alpha + \beta)}{1 - u^2(\alpha\beta + \alpha + \beta)} \end{aligned}$$

$$\text{At } \angle KY(p) = 180 \quad \cot \Phi = \infty, \text{ therefore } u^2 = \frac{1}{\alpha\beta + \alpha + \beta}$$

or $u_1 = \frac{1}{\sqrt{\alpha\beta + \alpha + \beta}}$. Then, as for (B)

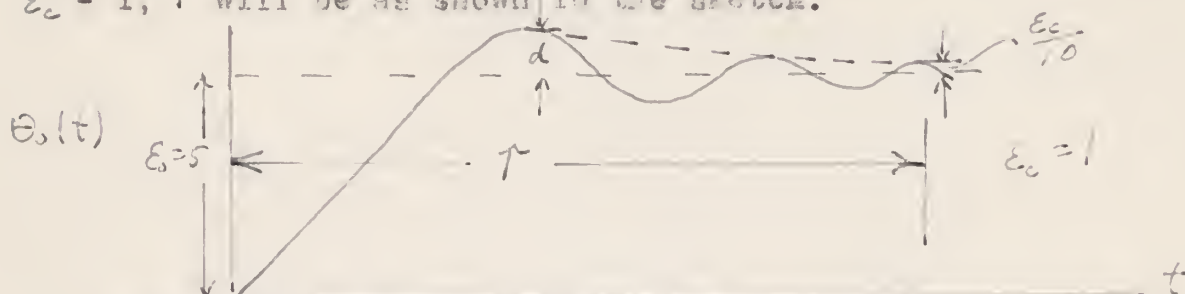
$$1 - (\text{gain margin}) = |KY(p)| = \frac{K \cos\theta_1 \cos\theta_2 \cos\theta_3}{u_1}$$

$$\begin{aligned} \text{where } \theta_1 &= \tan^{-1} u_1 \\ \theta_2 &= \tan^{-1} \alpha u_1 \\ \theta_3 &= \tan^{-1} \beta u_1 \end{aligned}$$

For expressions (B) and (C) values of α of 0.1 through 1.0, and β of 0.1 through 1.0 and phase margins of 15° , 30° , 45° , 60° , and 75° are considered. Curves of constant phase margin as a function of α vs. K are given for (B) and of β vs. K for values of $\alpha = .1, .4$, and $.8$ for (C). (Curves B-1, C-1 through C-4) Superimposed thereupon are curves of constant gain margins. These curves show the relation between gain and phase margins for the transfer functions considered. The low values of K associated with an uncompensated system are evident.

TRANSIENT RESPONSE

Of principal interest in the transient response to a step input of most servomechanisms are the amount of overshoot " d " and the time T required for the output of the system to arrive at or sufficiently near to the value of the input. Herein, time T will be the time required for the output of the system to arrive at one-tenth of the saturation value of the error signal. Since $\epsilon_c = 1$, T will be as shown in the sketch.

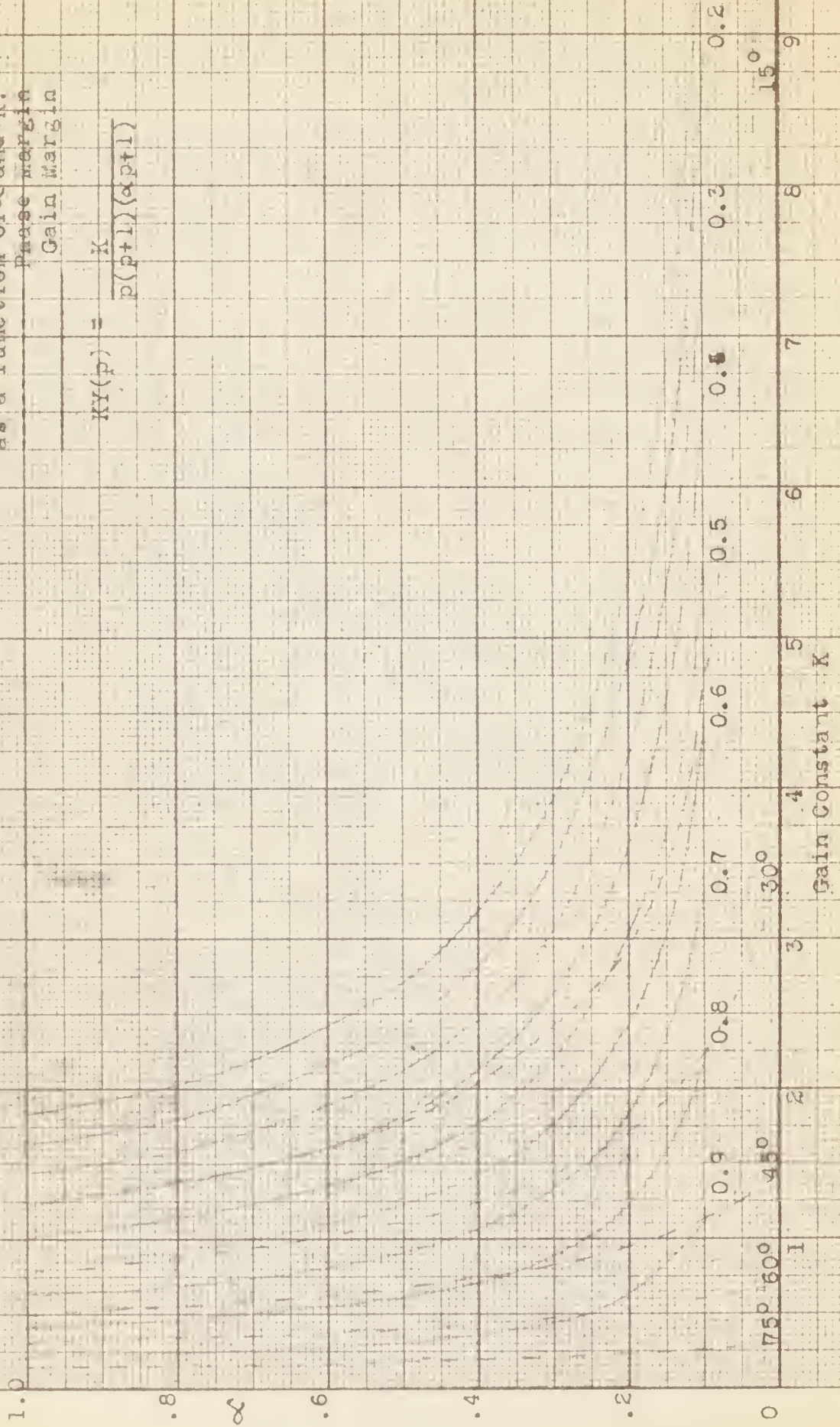


Curve B-2 gives the value of maximum overshoot " d " for the servo of expression (B) as a function of α . " d " is seen to vary more significantly with phase margin than with α . For phase margins of 45° and 60° " d " is essentially independent of α between $\alpha = .1$ and $\alpha = 1.0$.

Curve B-3 shows T , time to reach 1/10 saturation value of error signal as a function of α for various phase margins for the

Curve B-1
Phase Margin and Gain Margin
as a function of α and K.
Phase Margin
Gain Margin

$$XY(p) = \frac{K}{p(p+1)(\alpha p+1)}$$



Curve B-2

Maximum overshoot "d" as a function
of α . Phase Margin = $30^\circ, 45^\circ, 60^\circ$.

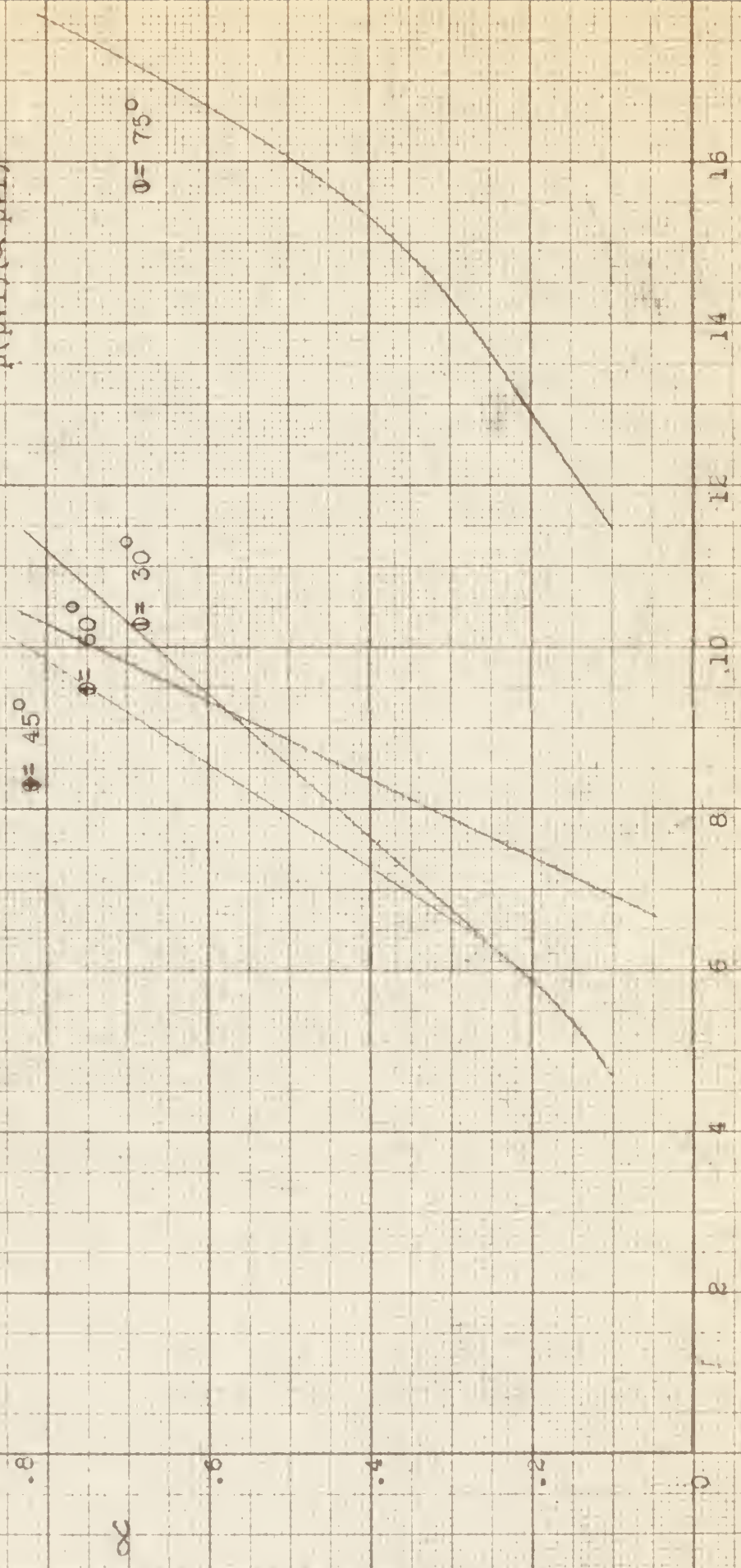
$$KX(p) = \frac{K}{p(p+1)(\alpha p+1)}$$



Curve B-3

Time τ for output to reach $\xi_c/10$
as a function of ϕ for phase
margin in $30^\circ, 45^\circ, 60^\circ, 75^\circ$.

$$KX(p) = \frac{K}{p(p+1)(\alpha p+1)}$$



Curve B-4

Maximum overshoot "d" vs. K. Phase
margin = 30°, 45°, 60°

$$KV(p) = \frac{K}{p(p+1)(\alpha p+1)}$$

1.25

1.0

.75

Maximum
overshoot
"d"

.50

.25

0

$\phi = 30^\circ$

$\phi = 45^\circ$

$\phi = 60^\circ$

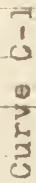
Gain Constant K

1

2

3

4

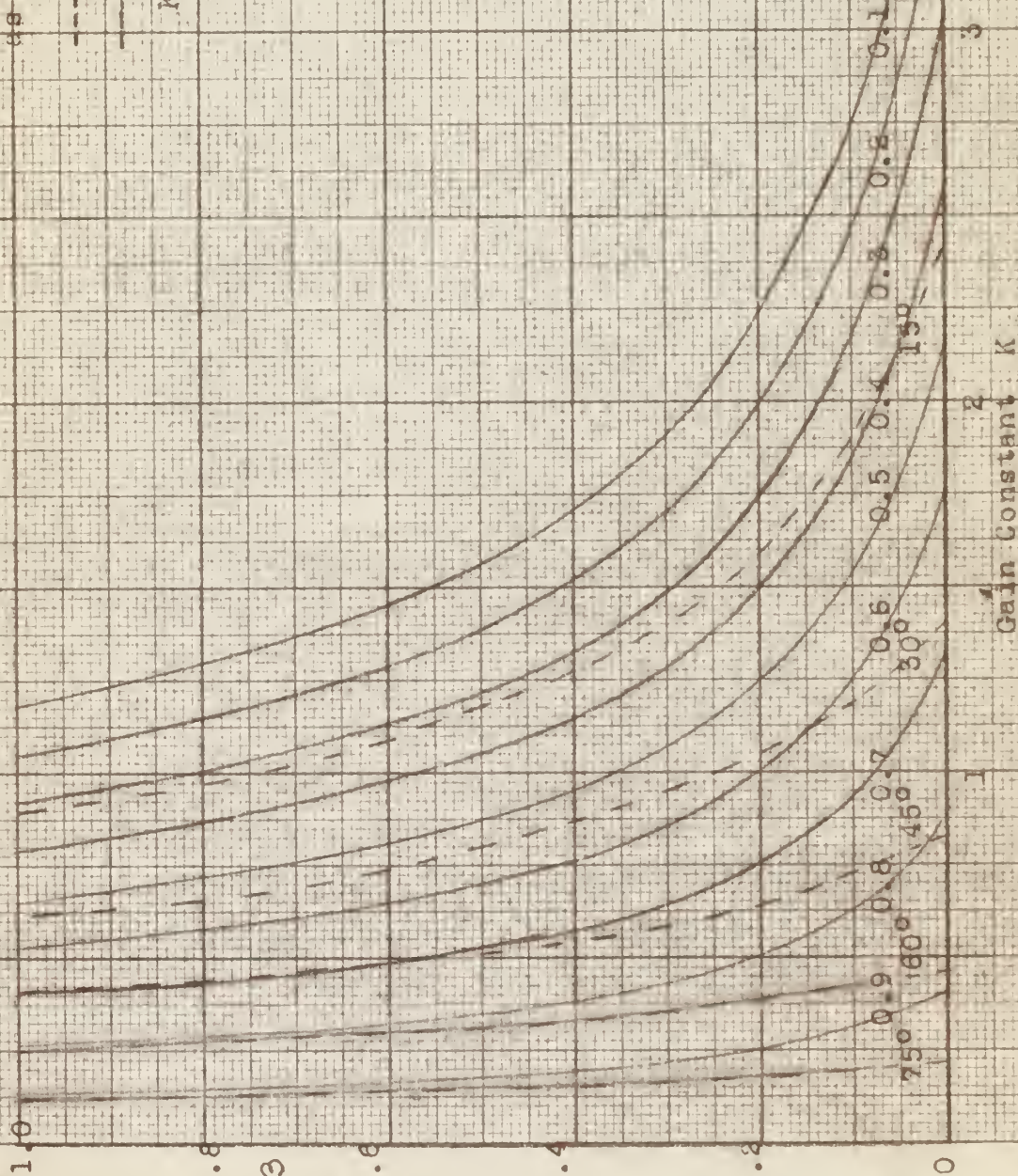


Curve C-8

Phase Margin and Gain Margin
as a function of θ and K for
 $\alpha = 0.3$

----- Phase Margin
----- Gain Margin

$$KX(p) = \frac{K}{p(p+1)(\alpha p+1)(\theta p+1)}$$



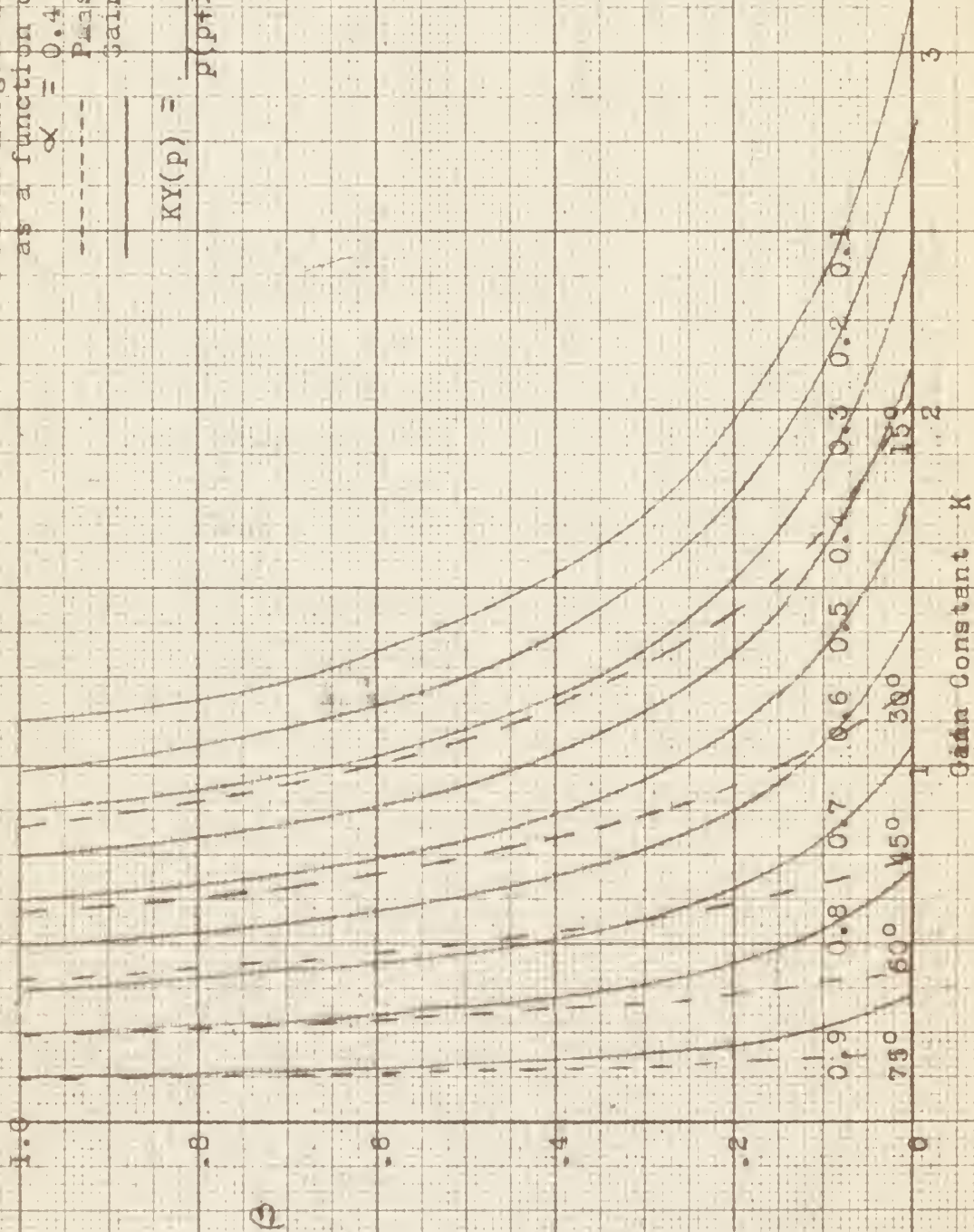
Curve C-3

Phase Margin and Gain Margin
as a function of β and K for

$$\alpha = 0.4$$

----- Phase Margin
_____ Gain Margin

$$KX(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$



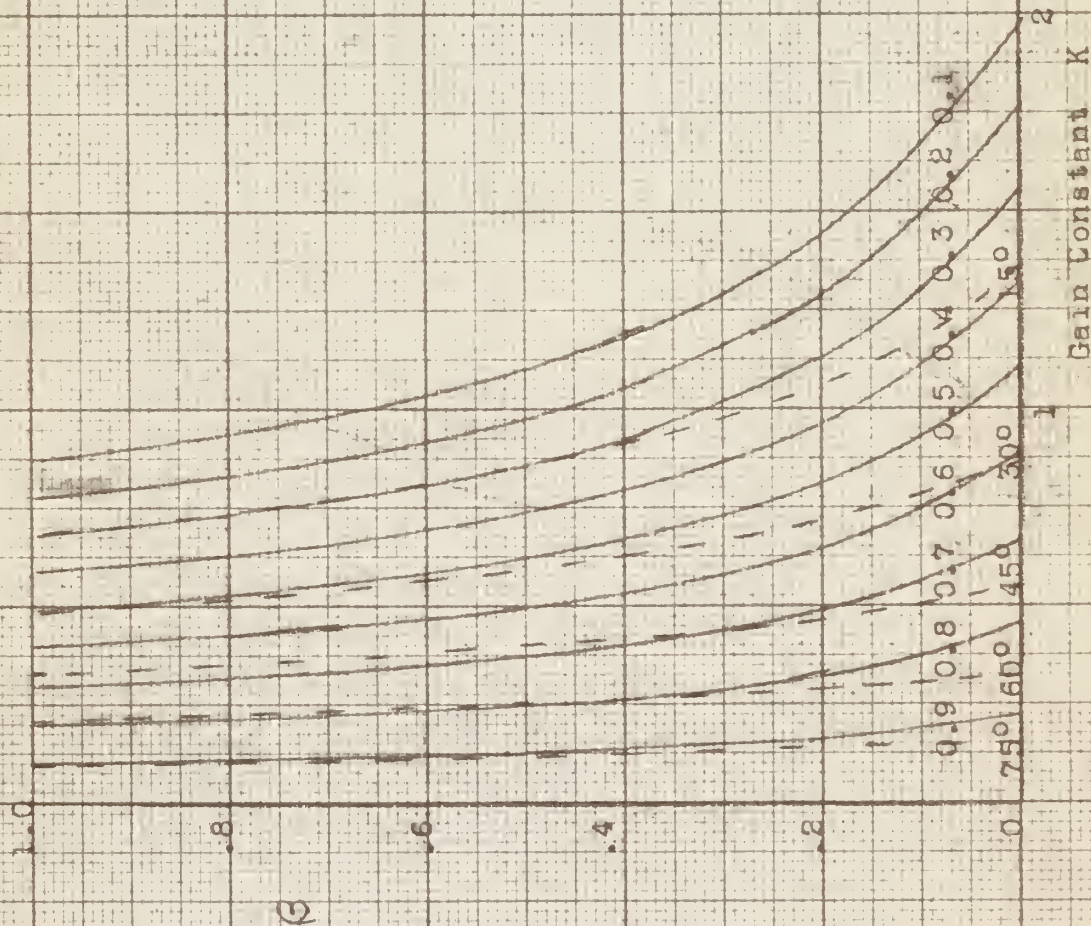
Curve C-4

Phase Margin and Gain Margin
as a function of θ and K for

$$\alpha = 0.8$$

----- Phase Margin
----- Gain Margin

$$KX(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$



servo of expression (B). There is evidently an optimum value of phase margin when τ is considered. Here a phase margin of 45° gives better response characteristics than does 30° or 60° . The servo is overdamped for phase margin of 75° . From this curve it appears that τ is dependent upon α , but for phase margins of $30^\circ - 60^\circ$, it is essentially independent of phase margin.

From Curve B-2 then, maximum overshoot d may be associated with phase margin while from Curve B-3 time τ for the servo to settle from its transient may be associated with α for values of phase margin of approximately $45^\circ - 60^\circ$.

Curve B-4 shows maximum overshoot d as a function of K for values of phase margin $\Phi = 30^\circ, 45^\circ, 60^\circ$. As would be expected from the similarity of the phase margin and maximum overshoot d curves versus α and K , this curve is almost a straight line.

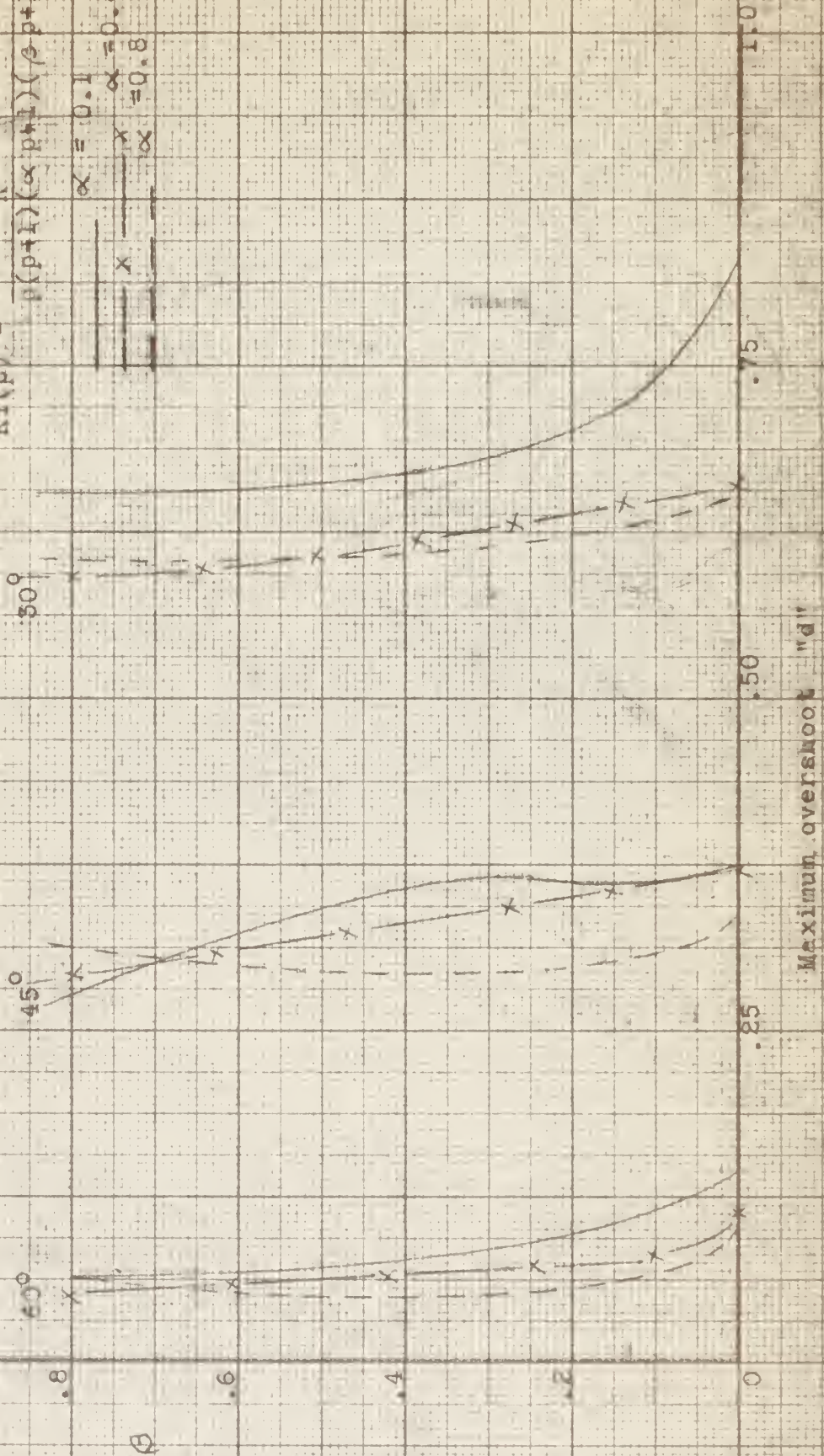
Curve C-5 shows maximum overshoot d for the various values of phase margin and β where $\alpha = 0.1, 0.4, 0.8$ in the servo of expression (C). Here d is essentially independent of both α and β but a function of Φ . This tendency was also shown in Curve B-2 for expression (B). Here again d may be associated with phase margin.

Curves C-6 through C-8 show τ as a function of β for $\alpha = 0.1, 0.4, 0.8$. τ is again essentially independent of phase margin though an optimum value of $\Phi = 60^\circ$ is indicated, for values of $\beta > 0.3$. τ increases with β for a given phase margin in a nearly linear fashion.

Curve C-5
Maximum overshoot "d" as a function
of β for Phase Margin 0°, 45°, 60°
where $\alpha = 0.1, 0.4, 0.8$.

$$KV(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$

$\alpha = 0.1$
 $\alpha = 0.4$
 $\alpha = 0.8$



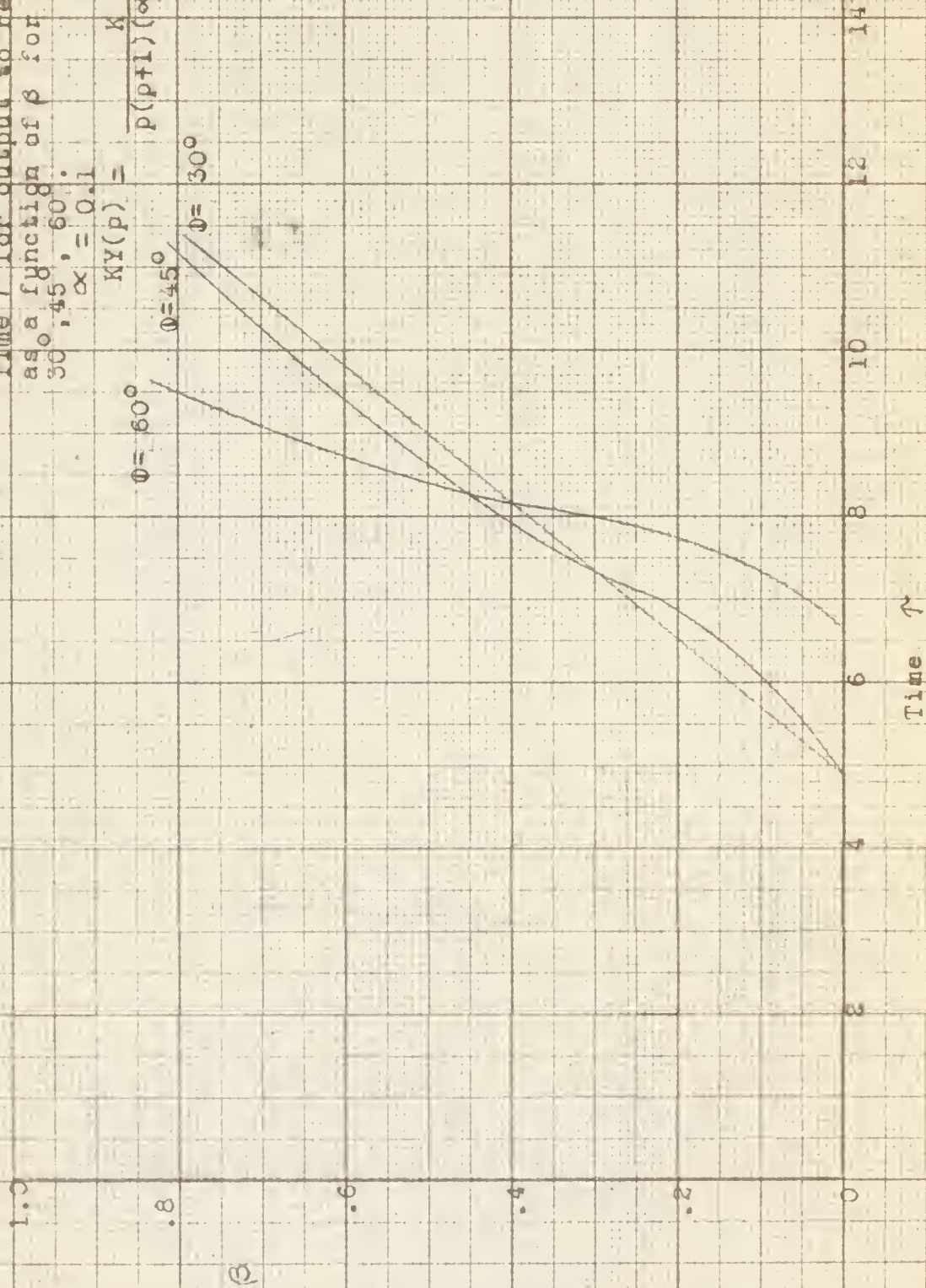
Curve C-6

Time τ for output to reach $E_c/10$
as a function of β for Phase Margin
30°, 45°, 60°.

$$\alpha = 0.1$$

$$KY(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$

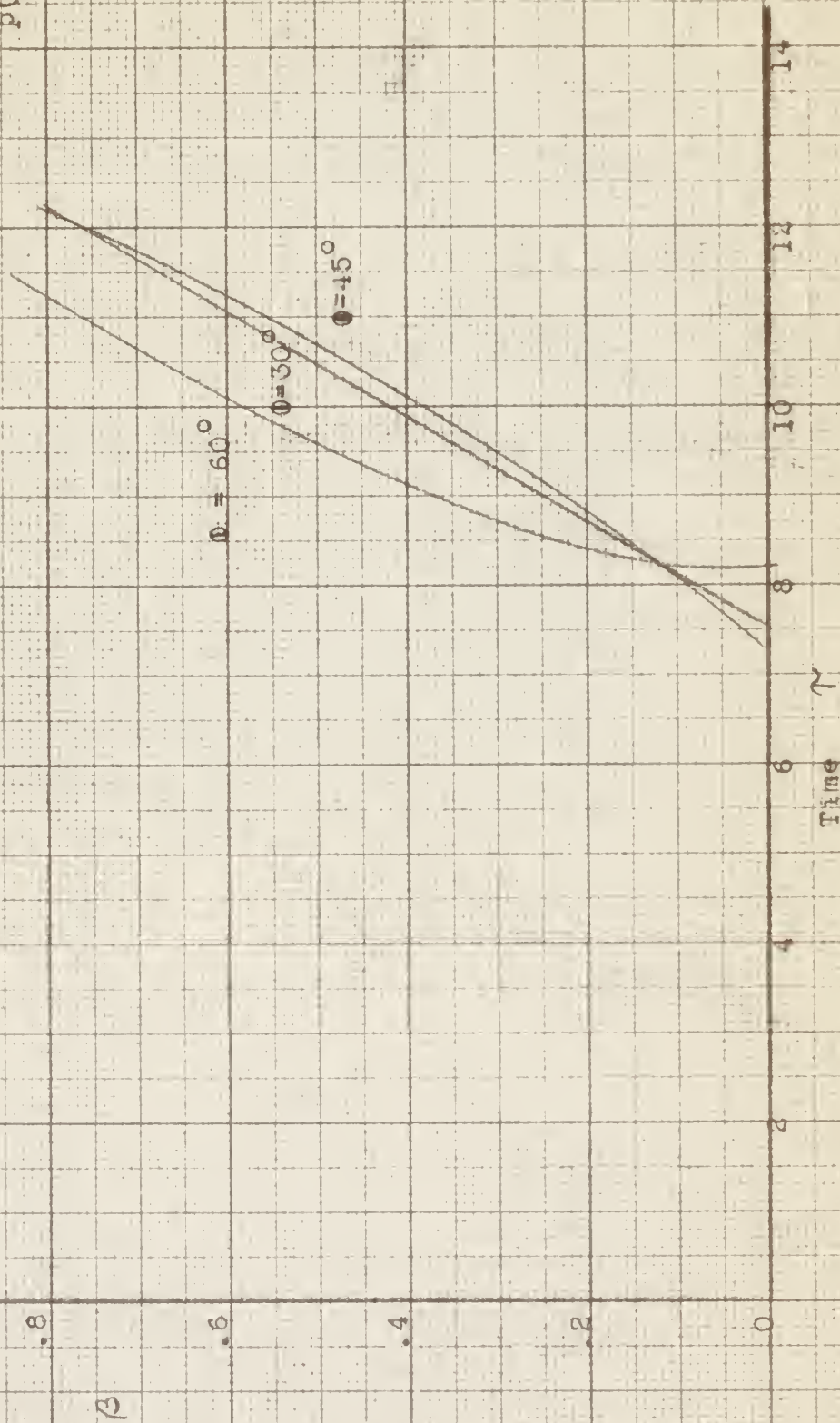
$\phi = 60^\circ$
 $\phi = 45^\circ$
 $\phi = 30^\circ$



Curve Q-7

Time τ for output to reach $\zeta_c/10$
 as a function of β for Phase Margin
 30°, 45°, 60°
 $\alpha = 0.4$

$$KY(p) = \frac{K}{p(p+1)(\alpha p+1)(\theta p+1)}$$



Curve C-8
Time for output to reach $\epsilon/10$
as a function of β for Phase Margin
30°, 45°, 60°
 $\alpha = 0.8$

$$XY(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$

$\theta = 60^\circ$
 $\theta = 45^\circ$
 $\theta = 30^\circ$

β

16

14

12

10

8

6

4

2

0

Time τ

In Curve C-9 \hat{T} is plotted vs. β for $\alpha = 0.1, 0.4, 0.8$. Phase margin was 45° in all cases. A dependence upon the values of both α and β is seen. This dependence was similarly noted in the servo having the transfer function of expression (D).

Curve D-1 shows transient response of the servos of expressions (B) and (C) for similar values of K . The runs paired together below had essentially the same transient response curves:

Run	KY(p)	Phase Margin			K
A-2	(B)	30°	.2	0	1.66
A-9	(C)	30°	.1	.1	1.65
B-16	(C)	60°	.4	.4	.316
B-28	(C)	60°	.2	.6	.316
B-2	(B)	45°	.4	0	.732
B-31	(C)	45°	.2	.2	.719
B-3	(B)	60°	.4	0	.400
B-24	(C)	60°	.2	.2	.414
B-2	(B)	30°	.3	.6	.731
B-53	(C)	30°	.1	.8	.732

As further comparison runs B-2, B-9, and B-16 are compared in Curve D-3.

B-2	(B)	45°	.4	0	.732
B-9	(C)	30°	.1	.8	.731
B-16	(C)	60°	.2	.6	.732

These runs, having similar K 's but different α, β or phase margins have very similar transient responses to a step input. While these results show equal values of K to give approximately the same transient responses for the servos of expressions (B) and (C) this result does not hold for that having the transfer function of expression (A). Thus in curve D-1, Run 10, $K = 0.732$, a different transient response results from that of Run B-16. Similarly, in Run A, use of a phase margin $\Phi = 30^\circ$ ($K = 3.16$)

Curve C-9

Time τ for output to reach $2\epsilon/10$
for $\alpha = 0.1, 0.4, 0.8$ as a function
of β . Phase Margin = 45° in all cases.

$$KX(p) = \frac{K}{p(p+1)(\alpha p+1)(\beta p+1)}$$

$\alpha = 0.1$ $\alpha = 0.4$

$\alpha = 0.8$

1.0

.8

.6

.4

.2

0

β

2

4

6

8

10

12

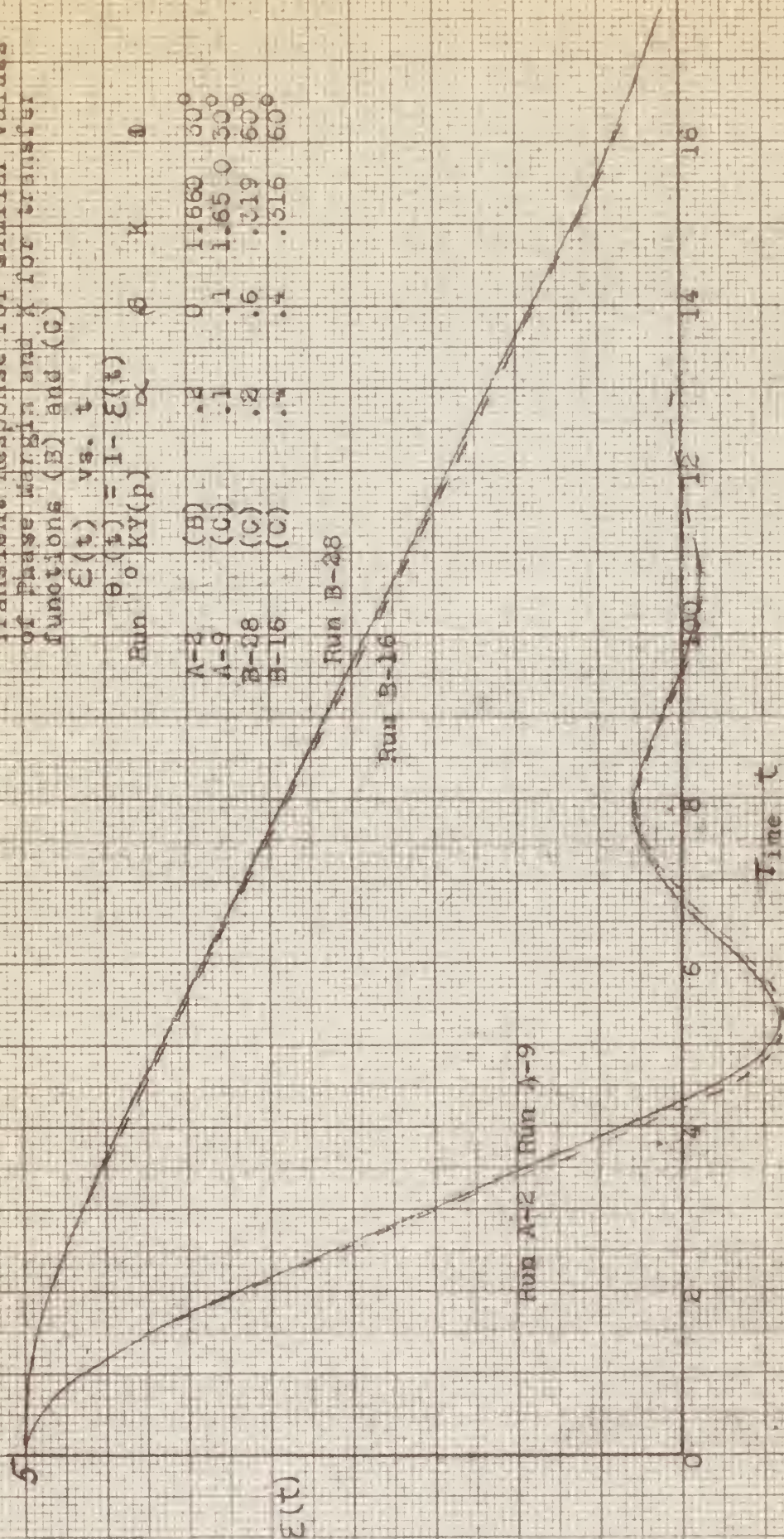
14

Time τ

Curve D-1

Transient Response for similar values
 of phase margin and K for transfer
 functions (B) and (C)

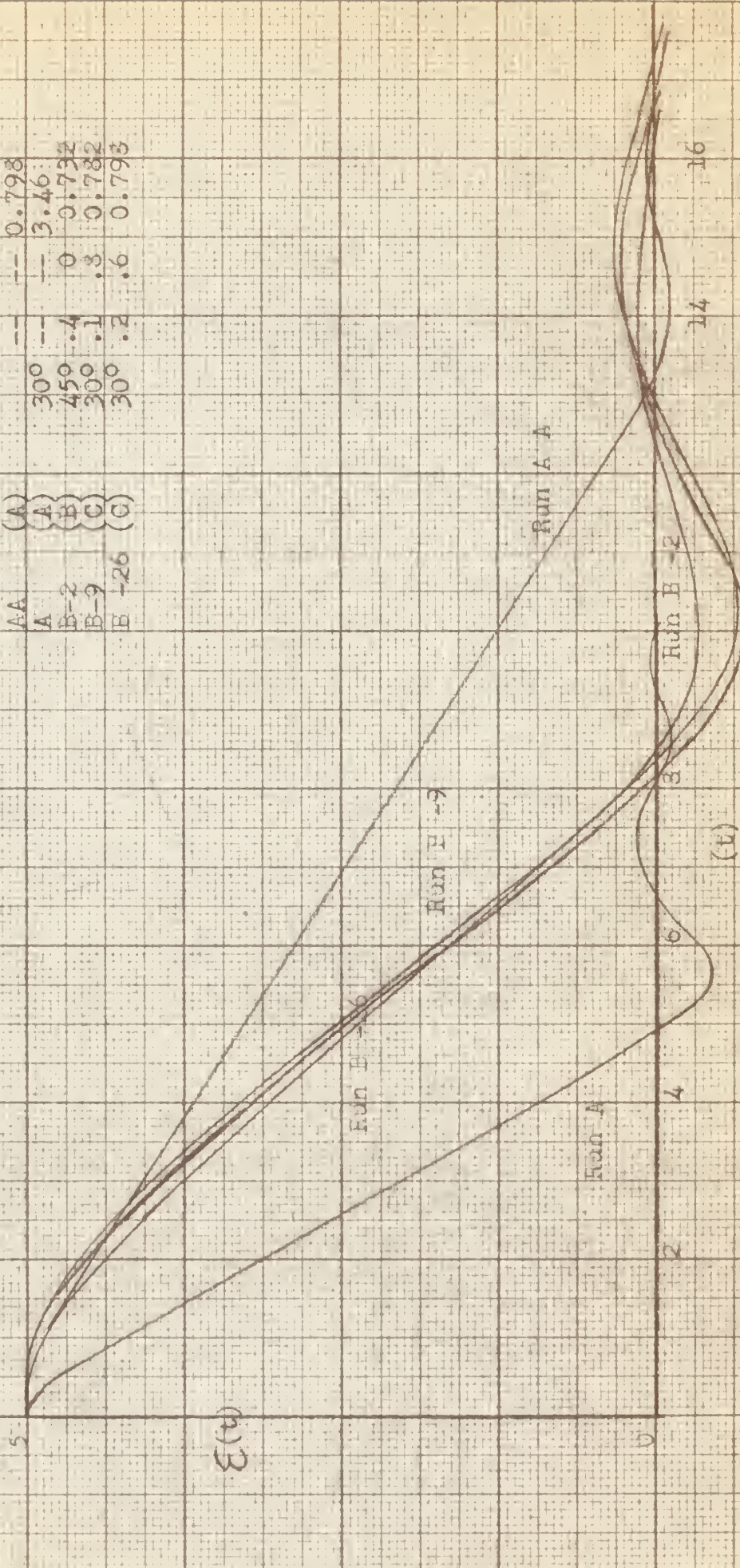
$\xi(t)$ vs. t	α	θ	K	ϕ
$\theta(t) = 1 - \xi(t)$				
Run A-2 (B)	.2	0	1.660	30°
A-9 (C)	.1	.1	1.650	30°
B-28 (C)	.2	.6	.219	60°
B-16 (C)	.4	.4	.316	60°



Curve D-2

Transient response, servos
of transfer functions (A), (B), (C).

Run	K _x (p)	θ	K
AA	(A)	--	0.798
A	(A)	30°	--
B-2	(B)	45°	0.732
B-3	(C)	30°	.1 .3 0.782
E-26	(C)	30°	.2 .6 0.793



in the servo of expression (A) gives a response different from that obtained in Run B-9 where a phase margin of 30° was also used.

Discussion

From the previous curves of phase margins as a function of α and β it is seen that where phase margin is large (60° - 75°) it is essentially linear with respect to K . For smaller values of phase margin this linearity no longer holds. For large values of α (or β) the curves of phase and gain margin are of similar shape. For small α (or β) this similarity ceases and for α (or β) in the vicinity $0 < \alpha$ or $\beta < 0.3$ there is marked dissimilarity. For transfer function (C) as α increases the curves of gain and phase margin become associated with smaller values of K .

The curves of maximum overshoot d as a function of α or β indicate that this property of the transient response may be associated with K . (It being understood however that K here is determined by α and β) The curves of time τ for the output to settle to a value $\epsilon_c/10$ indicate that τ may be associated with α or β .

The associations of maximum overshoot d with K , and of τ with α and β may be made analytically by reference to Ch. 11, ref (2).

There
$$h(t) = \frac{1}{\pi} \int_0^{\infty} \text{Re}(j\omega) \cos \omega t \, d\omega \quad \text{where} \quad H(j\omega) = \frac{\theta_o(j\omega)}{\theta_i(j\omega)} = \frac{KY(j\omega)}{1+KY(j\omega)}$$

Using the root plot of Fig. 2, Ch. 11 there may be obtained

$$\text{Re} \frac{KY}{1+KY} = \text{Re} \frac{\theta_o}{\theta_i} \quad \text{Here } \text{Re} \frac{\theta_o}{\theta_i} \text{ is determined by } K \text{ for a given } \alpha \text{ in expression (B) or a given } \alpha \text{ and } \beta \text{ in expression (C).}$$

Thus K determines the ordinate in the trapezoidal method given in Ch. 11 for the determination of the transient response and consequently determines d for a given servo system. Similarly, α and β determine the locations of the points w_1, w_2, \dots, w_n in this method and consequently the time τ for the transient response to settle to $\epsilon_c/10$.

The value of phase margin and of gain margin as design criteria is limited in that they each specify only one point on the transfer function locus. While useful in the discussion of a given servomechanism, their usefulness in synthesis of transfer functions must be augmented by more powerful methods, as for example the Lm and Ang vs $\log u$, $Lm-Ang$, KY^{-1} , and constant M constant N methods of ref (a).

Acknowledgments: The author wishes to acknowledge and express his appreciation of the assistance and suggestions of Dr. C. V. Veys, Jr., Moore School of Electrical Engineering, University of Pennsylvania, in the preparation of this paper.

Appendix (1)

NOMENCLATURE

θ_0 - output, controlled quantity

θ_1 - input, command quantity

ε - error, error signal

ε_c - value of error signal at which system saturates

ε_0 - input error signal, $\theta_1 - \theta_0$

K - gain constant

$KY(p)$ - transfer function

(p) - operator $p = ju$ in Laplace notation, $p = d/dt$ in differential notation.

τ - time required for transient to settle to $\varepsilon_c/10$

d - maximum overshoot of transient response

u - dimensionless frequency, $u = w \tau_1$

t - unit of time

τ_1 - largest time constant of transfer function

τ_2 - second largest time constant of transfer function

α = constant, τ_2/τ_1

β = constant, τ_2/τ_1

Appendix (2)

Bibliography

1. Reference (a) Principles of Servomechanisms - Brown and Campbell (Wiley)
2. Reference (b) Theory of Servomechanisms - Vol. 25, M.I.T. Radiation Laboratory Series (McGraw-Hill)
3. Reference (c) Network Analysis and Feedback Amplifier Design - Bode (Van Nostrand)
4. Reference (d) Transients in Linear Systems - Gardner and Barnes (Wiley)
5. Analysis and an Optimum Synthesis of Linear Servomechanisms - Herr and Geist #47-165 Vol.66 Trans. A.I.E.E.
6. Theory of Servomechanisms - Hazen Jour. Franklin Inst. Vol. 318 No.3 1934
7. Servomechanism Fundamentals - Leuer, Lesnick, Watson. (McGraw-Hill)
8. Linear Servo Theory - Graham Bell System Tech. Jour. October 1946

Thesis
H93

12627

William R. Jr.
nase margin and
e of some simple
Confidential

thesH93

Gain margin, phase margin and transient



3 2768 001 03587 6

DUDLEY KNOX LIBRARY